DESCRIPTION
The MPQ4570 is a frequency programmable step-down switching converter with integrated internal high-side and low-side power MOSFETs. It can provide 3A continuous output current with peak current control for excellent transient response and efficiency performance.

The wide 4.5V to 55V input voltage range accommodates a variety of step-down applications, including those applications in industrial, PoE, automotive and printer with DC high voltage bus.

The MPQ4570 uses peak current mode control to regulate the output voltage. The chip provides over current protection with valley current detection which is used to avoid current running way. Also it has accurate and reliable over voltage protection, and auto recovery thermal protection. In addition, the optional external soft start is available. Enable and power good indication function can be used to power track easily. In order to increase the efficiency, MPQ4570 will automatically scaling down the switching frequency when load is light. Meanwhile, the low side MOSFET will be turned off to reduce driver loss when zero inductor current is detected. MPQ4570 also features as a fully integrated solution with both high side and low side power MOSFETs. Synchronous operation mode with integrated low side MOSFET is much helpful to reduce the conduction loss and also beneficial to reduce external components space and save the cost.

The MPQ4570 is available in a TSSOP-20 EP with exposed pad package.

FEATURES
- Wide Input Voltage Range: 4.5V to 55V
- 90mΩ and 70mΩ Internal High and Low Power MOSFETs
- Peak Current Mode Control
- Programmable Switching Frequency
- Stable Independent on Output Capacitors
- Optional External Soft Start
- OCP Protection with Valley Current Detection
- Support External SYNC Clock
- OVP Protection
- Current Limit Decreasing during Output Short for Better Thermal Performance
- Power Good Indication
- Thermal Shutdown Protection
- Available in AEC-Q100 Grade 1

APPLICATIONS
- PoE Input Non-isolated Buck
- Industrial Power Systems
- Printers and Scanners
- Automotive Power Systems
- Distributed Power Systems

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TYPICAL APPLICATION

Efficiency vs. Load Current

V_{OUT}=5V

V_{IN}=12V

V_{IN}=24V

V_{IN}=36V

V_{IN}=48V

V_{IN}=65V

LOAD CURRENT (mA)

50 60 70 80 90 100

EFFICIENCY (%)
ORDERING INFORMATION

<table>
<thead>
<tr>
<th>Part Number</th>
<th>Package</th>
<th>Top Marking</th>
</tr>
</thead>
<tbody>
<tr>
<td>MPQ4570GF*</td>
<td>TSSOP-20 EP</td>
<td>See Below</td>
</tr>
<tr>
<td>MPQ4570GF-AEC1</td>
<td>TSSOP-20 EP</td>
<td>See Below</td>
</tr>
</tbody>
</table>

* For Tape & Reel, add suffix –Z (e.g. MPQ4570GF–Z);

TOP MARKING

MPSXYXY
MP4570
LLLLLLLLL

MP4570: product code of MPQ4570GF and MPQ4570GF-AEC1;
MPS: MPS prefix:
YY: year code;
WW: week code:
LLLLLLLLL: lot number;

PACKAGE REFERENCE

TOP VIEW

COMP 1
FB 2
FREQ 3
EN 4
BST 5
VIN 6
VIN 7
VIN 8
NC 9
SW 10

AGND 20
SS 19
PG 18
BIAS 17
VDD 16
GND 15
GND 14
GND 13
NC 12
SW 11

TSSOP-20 EP
ABSOLUTE MAXIMUM RATINGS (1)

Supply Voltage $V_{IN}$ ........................................... 60V
$V_{SW}$........................................... $-0.5V$ to $(VIN+0.5V)$
$V_{BS}$ ........................................... $V_{SW} + 6V$
All Other Pins................................. $-0.3V$ to $+6V$
EN Sink Current ................................. 150μA
Continuous Power Dissipation  
(TA = 25°C) (2) 
TSSOP-20 EP.................................. 2.78W
Junction Temperature ......................... 150°C
Lead Temperature ............................ 260°C
Storage Temperature ......................... $-65°C$ to $+150°C$

Recommended Operating Conditions
Supply Voltage $V_{IN}$ ......................... 4.5V to 55V
Output Voltage $V_{OUT}$ ........................ 1V to $0.9\cdot V_{IN}$
Operating Junction Temp. ($T_J$) ........................... $-40°C$ to $+125°C$

Thermal Resistance (3)  
$\theta_{JA}$  $\theta_{JC}$
TSSOP-20 EP .......................... 45 ...... 10... °C/W

Notes:
1) Absolute maximum ratings are rated under room temperature unless otherwise noted. Exceeding these ratings may damage the device.
2) The maximum allowable power dissipation is a function of the maximum junction temperature $T_J$ (MAX), the junction-to-ambient thermal resistance $\theta_{JA}$, and the ambient temperature $T_A$. The maximum allowable continuous power dissipation at any ambient temperature is calculated by $PD_{(MAX)} = (T_J{(MAX)}-T_A)/\theta_{JA}$. Exceeding the maximum allowable power dissipation will cause excessive die temperature, and the regulator will go into thermal shutdown. Internal thermal shutdown circuitry protects the device from permanent damage.
3) Measured on JESD51-7, 4-layer PCB.
### ELECTRICAL CHARACTERISTICS

\( V_{IN} = 48V, \ V_{EN} = 3.3V, \ T_{J} = -40^\circ C \) to \( +125^\circ C \), unless otherwise noted. Typical values are at \( T_{J} = 25^\circ C \).

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Condition</th>
<th>Min</th>
<th>Typ</th>
<th>Max</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td><strong>Error Amplifier</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Feedback Voltage</td>
<td>( V_{FB} )</td>
<td>( 4.5V \leq V_{IN} \leq 55V )</td>
<td>0.98</td>
<td>1</td>
<td>1.02</td>
<td>V</td>
</tr>
<tr>
<td>FB Current</td>
<td>( I_{FB} )</td>
<td>( V_{FB}=1.07V )</td>
<td>10</td>
<td>50</td>
<td></td>
<td>nA</td>
</tr>
<tr>
<td>Error AMP Transconductance</td>
<td></td>
<td></td>
<td>430</td>
<td>630</td>
<td>730</td>
<td>( \mu A/V )</td>
</tr>
<tr>
<td>COMP Sink/Source Current</td>
<td>( I_{COMP} )</td>
<td></td>
<td>13</td>
<td>30</td>
<td>52</td>
<td>( \mu A )</td>
</tr>
<tr>
<td><strong>Switch Characteristic</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Upper Switch On Resistance</td>
<td>( R_{ON,HS} )</td>
<td></td>
<td>90</td>
<td>160</td>
<td></td>
<td>( m\Omega )</td>
</tr>
<tr>
<td>Lower Switch On Resistance</td>
<td>( R_{ON,LS} )</td>
<td></td>
<td>70</td>
<td>120</td>
<td></td>
<td>( m\Omega )</td>
</tr>
<tr>
<td>Upper Switch Leakage</td>
<td>( I_{LKG,SW} )</td>
<td>( V_{EN} = 0V, \ V_{SW} = 0V )</td>
<td>10</td>
<td>300</td>
<td></td>
<td>nA</td>
</tr>
<tr>
<td><strong>Current Limit</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Peak Current Limit</td>
<td>( I_{LIMIT} )</td>
<td>( 10% ) Duty Cycle</td>
<td>3.9</td>
<td>5.7</td>
<td>7.5</td>
<td>A</td>
</tr>
<tr>
<td><strong>Quiescent Supply</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Quiescent Supply Current</td>
<td>( I_{Q} )</td>
<td>No load, Without Switching</td>
<td>450</td>
<td>670</td>
<td></td>
<td>( \mu A )</td>
</tr>
<tr>
<td>Shutdown Supply Current</td>
<td>( I_{SHDN} )</td>
<td>( V_{EN} = 0V )</td>
<td>7</td>
<td>18</td>
<td></td>
<td>( \mu A )</td>
</tr>
<tr>
<td><strong>VDD Regulator</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>VDD Regulator Output Voltage</td>
<td>( V_{DD} )</td>
<td>BIAS = NC</td>
<td>3.4</td>
<td>3.6</td>
<td>3.8</td>
<td>V</td>
</tr>
<tr>
<td>VDD Regulator Output Voltage</td>
<td>( V_{DD} )</td>
<td>BIAS = External 5V Power</td>
<td>4.6</td>
<td>4.8</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td><strong>Threshold Voltage</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>EN Rising Threshold</td>
<td>( V_{EN,R} )</td>
<td></td>
<td>1.4</td>
<td>1.6</td>
<td>1.8</td>
<td>V</td>
</tr>
<tr>
<td>EN Falling Threshold</td>
<td>( V_{EN,F} )</td>
<td></td>
<td>1.1</td>
<td>1.3</td>
<td>1.5</td>
<td>V</td>
</tr>
<tr>
<td>EN Threshold Hysteresis</td>
<td>( V_{EN,HYS} )</td>
<td></td>
<td>300</td>
<td></td>
<td></td>
<td>mV</td>
</tr>
<tr>
<td>VIN UVLO Rising Threshold</td>
<td>( V_{INUVR} )</td>
<td></td>
<td>3.7</td>
<td>3.9</td>
<td>4.1</td>
<td>V</td>
</tr>
<tr>
<td>VIN UVLO Falling Threshold</td>
<td>( V_{INUVF} )</td>
<td></td>
<td>3.3</td>
<td>3.5</td>
<td>3.7</td>
<td>V</td>
</tr>
<tr>
<td>VIN UVLO Threshold Hysteresis</td>
<td>( V_{INUHYS} )</td>
<td></td>
<td>400</td>
<td></td>
<td></td>
<td>mV</td>
</tr>
<tr>
<td><strong>Soft Start</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>External Soft Start Capacitor</td>
<td>( I_{SS} )</td>
<td>Charging Current ( V_{SS}=1V )</td>
<td>2.5</td>
<td>4</td>
<td>5.5</td>
<td>( \mu A )</td>
</tr>
<tr>
<td><strong>PWM Comparator</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Minimum Off Time (^{(4)})</td>
<td>( t_{OFF_MIN} )</td>
<td></td>
<td>100</td>
<td></td>
<td></td>
<td>ns</td>
</tr>
<tr>
<td>Minimum On Time (^{(4)})</td>
<td>( t_{ON_MIN} )</td>
<td></td>
<td>90</td>
<td></td>
<td></td>
<td>ns</td>
</tr>
</tbody>
</table>

\(^{(4)}\) Maximum duty cycle limited to 4%.
### ELECTRICAL CHARACTERISTICS (continued)

$V_{\text{IN}} = 48\text{V}$, $V_{\text{EN}} = 3.3\text{V}$, $T_J = -40^\circ\text{C}$ to $+125^\circ\text{C}$, unless otherwise noted. Typical values are at $T_J = 25^\circ\text{C}$.

<table>
<thead>
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<th>Parameter</th>
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<th>Min</th>
<th>Typ</th>
<th>Max</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td>Oscillator Frequency</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td>kHz</td>
</tr>
<tr>
<td>Switching Frequency</td>
<td>$f_{\text{SW}}$</td>
<td>$R_{\text{FREQ}}=100\text{k}$</td>
<td>400</td>
<td>520</td>
<td>640</td>
<td>kHz</td>
</tr>
<tr>
<td>OVP Protection</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Output OVP Threshold</td>
<td>$V_{\text{OVP}}$</td>
<td>$V_{\text{FB(OVP)}}/V_{\text{FB}}$</td>
<td>108</td>
<td>115</td>
<td>122</td>
<td>%</td>
</tr>
<tr>
<td>Power Good</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Power Good Threshold</td>
<td>$V_{\text{PG,TH}}$</td>
<td>$V_{\text{OUT Rising}}, V_{\text{FB(PG)}}/V_{\text{FB}}$</td>
<td>86</td>
<td>90</td>
<td>94</td>
<td>%</td>
</tr>
<tr>
<td></td>
<td>$V_{\text{PG,HYS}}$</td>
<td>$V_{\text{OUT Falling}}, V_{\text{FB(PG)}}/V_{\text{FB}}$</td>
<td>81</td>
<td>85</td>
<td>89</td>
<td>%</td>
</tr>
<tr>
<td></td>
<td>$t_{\text{PG,DLY}}$</td>
<td>$V_{\text{OUT Rising}}$</td>
<td>8</td>
<td>22</td>
<td>37</td>
<td>μs</td>
</tr>
<tr>
<td></td>
<td></td>
<td>$V_{\text{OUT Falling}}$</td>
<td>8</td>
<td>21</td>
<td>33</td>
<td>μs</td>
</tr>
<tr>
<td>Frequency SYNC</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>SYNC Leakage Current</td>
<td>$I_{\text{LKG,SYNC}}$</td>
<td></td>
<td>10</td>
<td>100</td>
<td></td>
<td>nA</td>
</tr>
<tr>
<td>SYNC Frequency Range</td>
<td>$f_{\text{SYNC}}$</td>
<td></td>
<td>100</td>
<td>1000</td>
<td></td>
<td>kHz</td>
</tr>
<tr>
<td>Thermal</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Thermal Shutdown (4)</td>
<td>$T_{\text{SD}}$</td>
<td></td>
<td>150</td>
<td>170</td>
<td></td>
<td>°C</td>
</tr>
<tr>
<td>Thermal Shutdown Hysteresis (4)</td>
<td>$T_{\text{SD,HYS}}$</td>
<td></td>
<td>10</td>
<td></td>
<td></td>
<td>°C</td>
</tr>
</tbody>
</table>

**Note:**

4) Derived from bench characterization. Not tested in production.
## PIN FUNCTIONS

<table>
<thead>
<tr>
<th>Pin #</th>
<th>Name</th>
<th>Description</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>COMP</td>
<td>Compensation Networks Setting. Please connect an external resistor series with a capacitor between this pin and GND.</td>
</tr>
<tr>
<td>2</td>
<td>FB</td>
<td>Feedback. This is the input to the PWM comparator. Please put an external resistive divider connected between the output and GND.</td>
</tr>
<tr>
<td>3</td>
<td>FREQ</td>
<td>Switching frequency setting pin. Connect a resistor from this pin to GND to set the switching frequency. If external SYNC clock is applied to this pin, the converter will follow this SYNC clock frequency.</td>
</tr>
<tr>
<td>4</td>
<td>EN</td>
<td>Enable Input. Pulling this pin below the specified threshold shuts the chip down. There is no internal pull-up or pull-down circuit, so do not float the pin.</td>
</tr>
<tr>
<td>5</td>
<td>BST</td>
<td>Bootstrap. This is the positive power supply for the internal floating high-side MOSFET driver. Connect a capacitor between this pin and SW pin.</td>
</tr>
<tr>
<td>6,7,8</td>
<td>VIN</td>
<td>Input Supply. This supplies power to all the internal control circuitry, VDD regulator. A decoupling capacitor to ground must be placed close to this pin to minimize switching spikes.</td>
</tr>
<tr>
<td>9,12</td>
<td>NC</td>
<td>Not connected pin. Please float this pin in the application.</td>
</tr>
<tr>
<td>10,11</td>
<td>SW</td>
<td>Switch Node. This is the output node from the internal high-side MOSFET source.</td>
</tr>
<tr>
<td>13,14,15, Exposed Pad</td>
<td>GND</td>
<td>Power ground pin for internal power MOSFETs.</td>
</tr>
<tr>
<td>16</td>
<td>VDD</td>
<td>Power for internal MOSFET driver and BST charging circuit.</td>
</tr>
<tr>
<td>17</td>
<td>BIAS</td>
<td>For better thermal performance, please connect this pin to external 5V source, VDD and internal circuit will be powered by BIAS. Since there is a diode inside between the BIAS pin and the internal circuit, please float this pin or connected to GND if not used.</td>
</tr>
<tr>
<td>18</td>
<td>PG</td>
<td>Power good indication. Please connect a resistor to a pull up power source if used.</td>
</tr>
<tr>
<td>19</td>
<td>SS</td>
<td>Optional external soft-start time setting. Connect an external capacitor between this pin and GND to set soft-start time externally. Floating the pin will activate the internal 0.5ms soft-start setting.</td>
</tr>
<tr>
<td>20</td>
<td>ANGD</td>
<td>Ground for internal logic and signal circuit.</td>
</tr>
</tbody>
</table>
TYPICAL CHARACTERISTICS

$V_{IN}=48V$, unless otherwise noted.

- **Feedback Voltage vs. Junction Temperature**
- **Quiescent Current vs. Junction Temperature**
- **Shutdown Current vs. Junction Temperature**
- **Current Limit vs. Junction Temperature**
- **Switch ON Resistance vs. Junction Temperature**
- **EN Threshold vs. Junction Temperature**
- **$V_{IN}$ UVLO vs. Junction Temperature**
- **$f_{SW}$ vs. Junction Temperature**
- **$I_{SS}$ vs. Junction Temperature**
TYPICAL CHARACTERISTICS

\( V_{IN} = 48 \text{V}, \text{unless otherwise noted.}\)
TYPICAL PERFORMANCE CHARACTERISTICS

\[ V_{\text{IN}} = 48V, \; V_{\text{OUT}} = 3.3V, \; C_{\text{OUT}} = 2 \times 22\mu F, \; L = 10\mu H, \; f_{\text{SW}} = 500kHz, \; T_A = +25^\circ C, \text{ unless otherwise noted.} \]

**Efficiency vs. Load Current**

- **VIN = 12V**
- **VIN = 24V**
- **VIN = 36V**
- **VIN = 48V**
- **VIN = 55V**

**Efficiency vs. Load Current**

- **VIN = 24V**
- **VIN = 12V**
- **VIN = 48V**
- **VIN = 36V**
- **VIN = 55V**

**Load Regulation**

- **VIN = 48V**
- **VIN = 12V**

**Line Regulation**

- **I_{OUT} = 1A**
- **I_{OUT} = 2A**
- **I_{OUT} = 3A**

\[ V_{\text{IN}} = 48V, \; V_{\text{OUT}} = 3.3V, \; C_{\text{OUT}} = 2 \times 22\mu F, \; L = 10\mu H, \; f_{\text{SW}} = 500kHz, \; T_A = +25^\circ C, \text{ unless otherwise noted.} \]
TYPICAL PERFORMANCE CHARACTERISTICS

$V_{IN} = 48V$, $V_{OUT} = 3.3V$, $C_{OUT} = 2 \times 22\mu F$, $L = 10\mu H$, $f_{SW} = 500kHz$, $T_A = +25^\circ C$, unless otherwise noted.
TYPICAL PERFORMANCE CHARACTERISTICS

\( V_{IN} = 48\, V, \quad V_{OUT} = 3.3\, V, \quad C_{OUT} = 2 \times 22\, \mu F, \quad L = 10\, \mu H, \quad f_{SW} = 500\, kHz, \quad T_A = +25^\circ C, \) unless otherwise noted.

**Shutdown Through EN**
- \( I_{OUT} = 0\, A \)

**SCP Entry**
- \( I_{OUT} = 3\, A \) to Short Circuit

**SCP Steady State**

**SCP Recovery**
- Short Circuit to \( I_{OUT} = 3\, A \)

**Load Transient**
- \( I_{OUT} = 1.5\, A \leftrightarrow 3\, A, \quad 1.6\, A/\mu s \)
Figure 1 — Functional Block Diagram
OPERATION

The MPQ4570 is a step-down switching regulator with integrated high-side high voltage power MOSFETs. It features as wide input voltage range, high efficiency, external internal soft-start, frequency programmable and comprehensive protection mode, i.e. OVP, OCP, OTP.

PWM Control

The MPQ4570 uses peak current mode control to regulate the output voltage.

A PWM cycle is initiated by the internal clock at the beginning of every cycle. After the high side MOSFET turns on, the inductor current will rise linearly to provide the energy to the load. The high side MOSFET remains on until its current hits the COMP voltage which is the output of the internal error amplifier (EA). The output voltage of error amplifier depends on the difference of output feedback voltage and the internal high precision reference and it will decide how much energy should be transferred to the load. The higher load current, the higher COMP voltage. After the high switch is off, the low side switch is on and the inductor current will flow through the low side switch. In order to avoid shoo-through issue, the dead time is inserted to avoid the high side and low side MOSFETS to turn on at the same time. For each turn on and off in a switching cycle, the high side MOSFET will keep on and off with minimum on and off time limit.

Light Load Operation

In order to get high efficiency, MPQ4570 has two features during light load: 1) When the load current decreases, the inductor current will drop at same time. The low side MOSFET will turn off in order to save driver loss when inductor current drops to zero. 2) When the load decreases, the switching frequency will be scaled down in order to reduce switching loss after COMP voltage drops down lower than certain threshold.

Error Amplifier

The error amplifier compares the FB pin voltage with the internal reference and outputs a current proportional to the difference between the two. This current is used to charge the external compensation networks to form the COMP voltage, which is used to control the high side up resistor requires limiting voltage amplitude to ≤6V to prevent damage to the zener diode. EN

MOSFET peak current and to regulate the output voltage.

Oscillator and SYNC Function

The internal oscillator frequency is set by a single external resistor \((R_{\text{FREQ}})\) connected between FREQ pin and GND. The frequency setting resistor should be located close to the device. The relationship between oscillator frequency and \(R_{\text{FREQ}}\) refer to table 1 in APPLICATION INFORMATION section.

During light load, the switching frequency will be scalded down according to the COMP voltage. The switching frequency will start to decrease when the COMP voltage is lower than around 0.8V. And the switching will be disabled when the COMP voltage drops lower than around 0.7V.

In order to reduce the switching loss and the thermal dissipation, the switching frequency will be decreased according to the FB voltage. When the FB is lower than 25%\(\times\)RFE, the switching frequency starts to decrease from the normal value, and finally drops to 5% of the normal value when the FB is zero.

The FREQ pin can be used to synchronize the internal oscillator rising edge to an external clock falling edge. Make sure the HIGH amplitude of SYNC clock is higher than 1.5V and LOW amplitude is lower than 1V to drive the internal logic. The recommended external SYNC frequency is in the range of 100kHz and 1MHz. There is no pulse width requirement but please note that there is always parasitic capacitance of the pad there, so, if the pulse width is too short, a clear rising and falling edge may not be seen due to the parasitic capacitance. The pulse longer than 100ns is recommended in application.

EN Control

EN is a control pin that turns the regulator on and off: Drive EN higher than 1.6V to turn on the regulator, drive it lower than 1.3V to turn off. There is no internal pull-up or pull-down at EN, so when it is floating, the EN status is uncertain.

The EN pin is clamped internally using a 6.5V zener diode between EN and GND, as shown in the functional block diagram. Connecting the EN pin directly to a voltage source without any pull-up resistor can be connected to higher voltage (e.g. VIN) through pull-up resistor if the system doesn’t
have another logic signal acting as enable signal. Just make sure the pull-up resistor is high enough to make sure the sink current into EN pin less than 150µA to avoid damaging the zener diode. For example, when connecting EN to \(V_{\text{IN}}=12\,\text{V}\), \(R_{\text{PULL-UP}} \geq (12\,\text{V} - 6.5\,\text{V}) \div 150\,\mu\text{A} = 37\,\text{k}\Omega\).

**Soft Start**

The soft start is implemented to ensure the smooth up output voltage during the power on and off. In addition, the soft start function also helps to reduce the inrush current value at the startup.

The soft start function is achieved by ramping SS up slowly and using SS to override the internal reference (REF) when SS-900mV is lower than REF. When SS-900mV is higher than REF, REF regains the control. The 900mV above is the offset voltage of SS which means SS is detected as 0 internally when it is lower than 900mV. To minimize the delay for SS to reach 0.9V, an internal pull-up circuit with about 30µA average current pulls SS up to 600mV first. Then use 4µA constant current to charge SS until it reaches to 2.5V. When SS is in the range of 0.9V to 1.9V, it overrides the REF as reference voltage of the error amplifier. During this period, output voltage ramps up from 0 to the regulated value following SS rising. The soft start time (\(t_{\text{SS}}\)) set by the external SS capacitor can be calculated by below formula:

\[
t_{\text{SS}}(\text{ms}) = \frac{C_{\text{SS}}(\text{nF}) \times V_{\text{REF}}(\text{V})}{I_{\text{SS}}(\mu\text{A})}
\]

Where \(C_{\text{SS}}\) is the external SS capacitor, \(V_{\text{REF}}\) is the internal reference voltage (1V), and \(I_{\text{SS}}\) is the 4 \(\mu\text{A}\) SS charge current.

The delay time for SS reaches to 900mV can be estimated as below:

\[
t_{\text{SS-delay}}(\text{ms}) = \frac{C_{\text{SS}}(\text{nF}) \times 0.6\text{V}}{30\,\mu\text{A}} + \frac{C_{\text{SS}}(\text{nF}) \times 0.3\text{V}}{4\,\mu\text{A}}
\]

There is also an internal fixed 500us soft start. The final SS time is determined by the longer time between 500µs and external SS setting time.

When output voltage is shorted to GND, feedback voltage is pulled to low then the SS will be discharged. The part will soft start again when the short at output is removed.

**Internal Regulator and BIAS**

There is an internal 2.5V regulator powers all the internal control circuits. The 2.5V regulator takes VIN as power supply when BIAS pin is lower than 3.2V while supplies from BIAS when BIAS is higher than 3.2V.

VDD regulator powers LS driver and also BST regulator when it is higher than 4.5V. VDD is powered from VIN when BIAS is floating and regulated at 3.6V. When BIAS is higher than 4.2V, it starts to power VDD. VDD will increases as BIAS rising with 600mV voltage drop and regulated at 4.8V when BIAS is higher than 5.4V. A 1µF decoupling capacitor is needed at the pin and make the capacitor as close to the pin as possible.

Using BIAS to power internal regulator can improve the efficiency. It is recommended to connect BIAS to an external power supply that is in the range of 3.3V to 5.5V. Output voltage is a good choice for this power supply if it is in above range. A 0.1µF to 1µF decoupling capacitor at the pin is recommended.

**Over Voltage Protection**

The MPQ4570 monitors the feedback output voltage to achieve the over voltage protection. If the FB voltage is higher than the 115%\(\times\)REF, the high side and low side MOSFET will be turned off immediately, the PG signal will be asserted to inform the fault status. High side and low side MOSFET will resume switching following close loop operation after FB voltage drops back to lower than 103%\(\times\)REF.

**Over Current Protection**

The MPQ4570 has cycle-by-cycle peak current limit protection and valley current detection protection. The inductor current is monitored during the high side MOSFET on state. If the inductor current exceeds the current limit value set by COMP voltage, the high side MOSFET turns off immediately. Then, the low side MOSFET will be turned on to discharge the energy and inductor current will decrease. The high side MOSFET will not be on again unless the inductor valley current is lower than a certain current threshold which is called the valley current limit. It is very useful to avoid the inductor current to run away. Also, both the peak current limit and the valley current limit value are
dependent on the FB voltage. If the feedback output voltage is higher than the 50% x REF, the current limit value is as the normal value. If the feedback output voltage is lower than 50% x RFF, the current limit will decrease and drop to the half normal value when the feedback output voltage is zero. This feature is very helpful to reduce the OCP thermal dissipation which may especially get worse when the output voltage is shorted. Also, it is very helpful to reduce the high inrush current during the startup.

**UVLO Protection**

The MPQ4570 has input under voltage lockout protection (UVLO). Assuming the EN is active, the MPQ4570 is powered on when the input voltage is higher than the UVLO rising threshold and is powered off when input voltage drops below the UVLO falling threshold.

**Thermal Shutdown Protection**

The thermal shutdown is employed in MPQ4570 by monitoring the IC temperature internally. If the junction temperature exceeds the threshold (typically 170°C), the regulator shuts off and it will turn on again when the temperature drops below 160°C. There is a ~10°C hysteresis.

**Power Good**

MPQ4570 has one power good (PG) pin out to indicate the normal operation after soft start time. The PG pin is the open drain of an internal MOSFET. It should be connected to VDD or external voltage source through a resistor (i.e. 100kohm). After the input voltage is applied, the MOSFET is turned on and the PG pin is pulled to GND before SS is ready. After the FB voltage reaches 90% REF voltage, the MOSFET turns off and PG pin is pulled to high by external voltage source. When the FB voltage drops to 85% REF voltage, the PG voltage is pulled to GND to indicate a failure output status.

**Floating Driver and Bootstrap Charging**

An external bootstrap capacitor (0.1µF typically) between BST pin and SW pin powers the floating power MOSFET driver. This floating driver has its own UVLO protection. This UVLO's rising threshold is 2.3V with a hysteresis of 300mV. The driver's UVLO is soft-start related: When the bootstrap voltage hits its UVLO threshold, the soft-start circuit resets. When bootstrap UVLO is gone, the reset is off and then the soft-start process resumes.

The dedicated internal bootstrap regulator regulates and charges the bootstrap capacitor to 4.2V. When the voltage between the BST and SW nodes is less than its regulation, a PMOS pass transistor from VIN to BST turns ON. The charging current path is from VIN, BST and then to SW.

As long as V IN is sufficiently higher than V SW, the bootstrap capacitor can be charged. When the high side MOSFET is ON, V IN=V SW so the bootstrap capacitor can’t be charged. When low side MOSFET is ON, the difference between V IN and V SW is at its largest, thus making it the best period to charge. When there is no current in the inductor, V SW=V OUT so the difference between V IN and V OUT can charge the bootstrap capacitor.

At higher duty cycles, the time period available for bootstrap charging is shorter so the bootstrap capacitor may not be sufficiently charged. If the internal circuit does not have sufficient voltage and the bootstrap capacitor is not charged, extra external circuitry can be used to ensure the bootstrap voltage is within the normal operational region.
APPLICATION INFORMATION

COMPONENT SELECTION

Setting the Switching Frequency

The MPQ4570 has an externally adjustable frequency. The switching frequency \( f_{SW} \) can be set using a resistor at FREQ pin \( R_{FREQ} \). The recommended \( R_{FREQ} \) values for various \( f_{SW} \) see table1. Refer to \( f_{SW} \) vs. \( R_{FREQ} \) curve in TYPICAL CHARACTERISTICS section for more detailed values.

<table>
<thead>
<tr>
<th>( f_{SW} ) (kHz)</th>
<th>( R_{FREQ} ) (kΩ)</th>
</tr>
</thead>
<tbody>
<tr>
<td>1000</td>
<td>47.5</td>
</tr>
<tr>
<td>900</td>
<td>56</td>
</tr>
<tr>
<td>800</td>
<td>63.4</td>
</tr>
<tr>
<td>700</td>
<td>73.2</td>
</tr>
<tr>
<td>600</td>
<td>84.5</td>
</tr>
<tr>
<td>500</td>
<td>102</td>
</tr>
<tr>
<td>400</td>
<td>133</td>
</tr>
<tr>
<td>300</td>
<td>178</td>
</tr>
<tr>
<td>200</td>
<td>261</td>
</tr>
<tr>
<td>100</td>
<td>523</td>
</tr>
</tbody>
</table>

Setting the Output Voltage

A resistive voltage divider from the output voltage to FB pin sets the output voltage. The voltage divider divides the output voltage down to the feedback voltage by the ratio:

\[
V_{FB} = V_{OUT} \times \frac{R_2}{R_1 + R_2}
\]

Thus the output voltage is:

\[
V_{OUT} = V_{FB} \times \frac{R_1 + R_2}{R_2}
\]

For example, the value for \( R_1 \) can be 10kΩ. With this value, \( R_2 \) is:

\[
R_2 = \frac{10}{V_{OUT} - 1}\kOmega
\]

So for a 3.3V output voltage, \( R_1 \) is 10kΩ, and \( R_1 \) is 4.32kΩ.

Inductor

The inductor provides constant current to the output load while being driven by the switched input voltage. A larger-value inductor will result in lower ripple current that will lower the output ripple voltage. However, a larger inductor value will be physically larger, have higher series resistance, or lower saturation current.

To determine the inductance, allow the inductor’s peak-to-peak ripple current to approximately equal 30% of the maximum switch current limit. Make sure that the peak inductor current is less than the maximum switch current limit. The inductance value can be calculated by:

\[
L_1 = \frac{V_{OUT}}{f_{SW} \times \Delta I_L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)
\]

Where \( V_{OUT} \) is the output voltage, \( V_{IN} \) is the input voltage, \( f_S \) is the switching frequency, and \( \Delta I_L \) is the peak-to-peak inductor ripple current.

Choose an inductor that will not saturate under the maximum inductor peak current. The peak inductor current can be calculated by:

\[
I_{LP} = I_{LOAD} + \frac{V_{OUT}}{2 \times f_{SW} \times L_1} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)
\]

Where \( I_{LOAD} \) is the load current.

Input Capacitor

The input current to the step-down converter is discontinuous and requires a capacitor to supply the AC current to the step-down converter while maintaining the DC input voltage. Use capacitors with low equivalent series resistances (ESR) for the best performance. Ceramic capacitors are best, but tantalum or low-ESR electrolytic capacitors may also suffice.

For simplification, choose the input capacitor with an RMS current rating greater than half of the maximum load current. The input capacitor (C1) can be electrolytic, tantalum, or ceramic.

When using electrolytic or tantalum capacitors, place a small, high-quality, ceramic capacitor (0.1μF) as close to the IC as possible. When using ceramic capacitors, make sure that they have enough capacitance to provide sufficient charge to prevent excessive voltage ripple at the input. The input voltage ripple caused by capacitance is approximately:
\[ \Delta V_{\text{IN}} = \frac{I_{\text{LOAD}}}{f_{\text{SW}} \times C1} \times \frac{V_{\text{OUT}}}{V_{\text{IN}}} \times \left(1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}} \right) \]

**Output Capacitor**

The output capacitor (C2) maintains the DC output voltage. Use ceramic, tantalum, or low-ESR electrolytic capacitors. Low-ESR capacitors are preferred to keep the output voltage ripple low. The output voltage ripple can be estimated as:

\[ \Delta V_{\text{OUT}} = \frac{V_{\text{OUT}}}{f_{\text{SW}} \times L} \times \left(1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}} \right) \times \left(1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}} \right) \times \frac{1}{R_{\text{ESR}} + \frac{1}{8 \times f_{\text{SW}} \times C2}} \]

Where L is the inductor value and \( R_{\text{ESR}} \) is the ESR value of the output capacitor.

For ceramic capacitors, the capacitance dominates the impedance at the switching frequency and contributes the most to the output voltage ripple. For simplification, the output voltage ripple can be estimated by:

\[ \Delta V_{\text{OUT}} = \frac{V_{\text{OUT}}}{8 \times f_{\text{SW}} \times L \times C2} \times \left(1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}} \right) \]

For tantalum or electrolytic capacitors, the ESR dominates the impedance at the switching frequency. For simplification, the output ripple is approximately:

\[ \Delta V_{\text{OUT}} = \frac{V_{\text{OUT}}}{f_{\text{SW}} \times L} \times \left(1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}} \right) \times R_{\text{ESR}} \]

The characteristics of the output capacitor also affect the stability of the regulation system. The MPQ4570 can be optimized for a wide range of capacitances and ESR values.

**Compensation Components**

MPQ4570 employs current-mode control for easy compensation and fast transient response. The COMP pin controls the system stability and transient response. The COMP pin is the output of the internal error amplifier. A series capacitor-resistor combination sets a pole-zero combination to control the control system’s characteristics. The DC gain of the voltage feedback loop is:

\[ A_{\text{VDC}} = R_{\text{LOAD}} \times G_{\text{CS}} \times A_{\text{VEA}} \times \frac{V_{\text{FB}}}{V_{\text{OUT}}} \]

Where \( A_{\text{VEA}} \) is the error-amplifier voltage gain, \( 1000 \text{V/V} \); \( G_{\text{CS}} \) is the current-sense transconductance, \( 12 \text{A/V} \); \( R_{\text{LOAD}} \) is the load resistor value.

The system has two important poles: One from the compensation capacitor (C3) and the output resistor of error amplifier, and the other due to the output capacitor and the load resistor. These poles are located at:

\[ f_{p1} = \frac{G_{\text{EA}}}{2 \pi \times C3 \times A_{\text{VEA}}} \]

\[ f_{p2} = \frac{1}{2 \pi \times C2 \times R_{\text{LOAD}}} \]

Where, \( G_{\text{EA}} \) is the error-amplifier transconductance, \( 630 \mu \text{A/V} \).

The system may have another significant zero if the output capacitor has a large capacitance or a high ESR value. This zero is located at:

\[ f_{z1} = \frac{1}{2 \pi \times C3 \times R3} \]

In this case, a third pole set by the compensation capacitor (C4) and the compensation resistor can compensate for the effect of the ESR zero. This pole is located at:

\[ f_{p3} = \frac{1}{2 \pi \times C4 \times R3} \]

The goal of compensation design is to shape the converter transfer function for a desired loop gain. The system crossover frequency where the feedback loop has unity gain is important: Lower crossover frequencies result in slower line and load transient responses, while higher crossover frequencies lead to system instability. Generally, set the crossover frequency to \( \approx 0.1 \times f_{\text{SW}} \).
Follow these steps to design the compensation:

1. Choose $R_3$ to set the desired crossover frequency:

$$R_3 = \frac{2\pi \times C_2 \times f_C \times V_{OUT}}{G_{EA} \times G_{CS} \times V_{FB}}$$

Where $f_C$ is the desired crossover frequency.

2. Choose $C_3$ to achieve the desired phase margin. For applications with typical inductor values, set the compensation zero ($f_{Z1}$) < 0.25 $\times f_C$ to provide sufficient phase margin. $C_3$ is then:

$$C_3 > \frac{4}{2\pi \times R_3 \times f_C}$$

3. $C_4$ is required if the ESR zero of the output capacitor is located at <0.5 $\times f_{SW}$, or the following relationship is valid:

$$\frac{1}{2\pi \times C_2 \times R_{ESR}} < \frac{f_{SW}}{2}$$

If this is the case, use $C_4$ to set the pole ($f_{P3}$) at the location of the ESR zero. Determine the $C_4$:

$$C_4 = \frac{C_2 \times R_{ESR}}{R_3}$$

**External Bootstrap Diode**

For high duty-cycle operation (when $V_{OUT}/V_{IN}$ > 65%), the time period available to the bootstrap charging is less so the bootstrap capacitor may not be charged sufficiently. This affects the efficiency, even the normal operation of the part. An external bootstrap diode from 3V-5V rail to the BST pin can help to charge the bootstrap capacitor and enhance the efficiency. Output voltage is the good choice of this power supply if it is in above range. The bootstrap diode can be a low cost one such as IN4148.

At no-load or light-load, the converter may operate in pulse-skipping mode in order to maintain output-voltage regulation. Under this condition, $V_{SW}=V_{OUT}$ in most time period, so the diode from $V_{OUT}$ to BST can’t charge the bootstrap capacitor. For sufficient gate voltage during pulse-skipping, $V_{IN}=V_{OUT}$ should be no less than 3V. For example, if the $V_{OUT}=3.3V$, $V_{IN}$ must exceed 3.3V+3V=6.3V to maintain sufficient bootstrap voltage at no-load or light-load. To meet this requirement, the EN pin can program the input UVLO voltage to $V_{OUT}$+3V

**PCB Layout Guide**

PCB layout is very important to stable operation. Please follow below guidelines and use figure 3 as reference.

1. Place the ceramic input capacitor as close to IN and GND pins as possible, especially the small package size (0603) input bypass capacitor. Keep the connection of input capacitor and IN pin as short and wide as possible.

2. Place the $V_{DD}$ capacitor to $V_{DD}$ pin and GND pin as close as possible.

3. Use large ground plane directly connect to GND pin. Add vias near the GND pin if bottom layer is ground plane.

4. Route SW, BST away from sensitive analog areas such as FB.

5. Ensure all feedback connections are short and direct. Place the feedback resistors as close to the chip as possible.

6. Connect IN, SW, and especially GND and exposed pad to large copper areas to cool the chip for improved thermal performance and long-term reliability.

**Figure 2 — External Bootstrap Diode**
Figure 3 – Recommended PCB Layout

Top Layer

Inner 1 Layer

Inner 2 Layer

Bottom Layer
TYPICAL APPLICATION CIRCUITS

Figure 4 – 3.3V Output Typical Application Circuit
PACKAGE INFORMATION

TSSOP-20 EP
(EXPOSED PAD)

TOP VIEW

RECOMMENDED LAND PATTERN

FRONT VIEW

SIDE VIEW

DETAIL "A"

NOTE:

1) ALL DIMENSIONS ARE IN MILLIMETERS.
2) PACKAGE LENGTH DOES NOT INCLUDE MOLD FLASH, PROTRUSION OR GATE BURR.
3) PACKAGE WIDTH DOES NOT INCLUDE INTERLEAD FLASH OR PROTRUSION.
4) LEAD COPLANARITY (BOTTOM OF LEADS AFTER FORMING) SHALL BE 0.10 MILLIMETERS MAX.
5) DRAWING CONFORMS TO JEDEC MO-153, VARIATION ACT.
6) DRAWING IS NOT TO SCALE.

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