DESCRIPTION
The MP024-10 is a low-cost, offline, primary-side, flyback regulator with a simple, external circuit. It provides accurate constant voltage (CV) and constant current (CC) regulation without an optocoupler or secondary feedback circuit and has an integrated 700V MOSFET and high-voltage start-up current source.

The MP024-10 operates in discontinuous conduction mode (DCM) using variable off-time control. Its power-saving technologies limit the no-load power consumption to less than 30mW.

Full protection features include VCC under-voltage lockout (VCC UVLO), overload protection (OLP), over-temperature protection (OTP), open-loop protection (OCP), sensing short protection (SSP), and over-voltage protection (OVP).

The variable switching frequency method provides natural spectrum shaping to smooth the EMI signature, making the MP024-10 suitable for offline, low-power battery chargers and adapters.

The MP024-10 is available in a SOIC8-7B package.

<table>
<thead>
<tr>
<th>Maximum Output Power</th>
<th>230Vac ±15%</th>
<th>85Vac~265Vac</th>
</tr>
</thead>
<tbody>
<tr>
<td>Open Frame (2)</td>
<td>13</td>
<td>10</td>
</tr>
<tr>
<td>Adapter (3)</td>
<td>10</td>
<td>7.5</td>
</tr>
</tbody>
</table>

NOTES:
1) The maximum output power is limited by thermal shutdown.
2) Maximum continuous power in an open frame design at 50°C ambient temperature.
3) Maximum continuous power in a non-ventilated enclosed adapter measured at 50°C ambient temperature.
4) Single output, $V_{OUT} = 5V$. 

FEATURES
- Primary-Side Control without Optocoupler or Secondary Feedback Circuit
- Precise Constant Current and Constant Voltage Control (CC/CV)
- Variable Off-Time Peak-Current Control
- 700V/4.5Ω Integrated MOSFET
- 700V High-Voltage Current Source
- 30mW No-Load Power Consumption
- Programmable Cable Compensation
- Multiple Protections: OVP, OCP, SSP, OLP, OTP, and VCC UVLO
- Low Cost and Simple External Circuit
- Available in a SOIC8-7B Package

APPLICATIONS
- Cell Phone Chargers
- Adapters for Handheld Electronics
- Standby and Auxiliary Power Supplies

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TYPICAL APPLICATION

![Diagram of MP024-10 Primary-Side CC/CV Regulator]
ORDERING INFORMATION

<table>
<thead>
<tr>
<th>Part Number*</th>
<th>Package</th>
<th>Top Marking</th>
</tr>
</thead>
<tbody>
<tr>
<td>MP024GS-10</td>
<td>SOIC8-7B</td>
<td>See Below</td>
</tr>
</tbody>
</table>

* For Tape & Reel, add suffix –Z (e.g. MP024GS-10–Z)

TOP MARKING

MP024-10
LLLLLLLLL
MPSYWW

MP024-10: First five digits of the part number
LLLLLLLLL: Lot number
MPS: MPS prefix
Y: Year code
WW: Week code

PACKAGE REFERENCE
ABSOLUTE MAXIMUM RATINGS (5)
DRAIN to SOURCE, GND ........... -0.3V to 700V
VCC to GND .................................. -0.3V to 28V
CP, SS, SOURCE to GND ........... -0.3V to 7V
FB to GND .................................... -0.7V to 7V
Continuous power dissipation (T_A = +25°C) (6)
...................................................... 1.66W
Junction temperature .................. 150°C
Lead temperature ....................... 260°C
Storage temperature ............... -60°C to +150°C
ESD capability human body model ... 2.0kV
ESD capability machine model .......... 200V

Recommended Operating Conditions (7)
Junction temperature (T_J) .......... -40°C to +125°C
Ambient temperature (T_A) .......... -40°C to +110°C
Operating VCC range ............... 10V to 25V

Thermal Resistance (4) θJA θJC
SOIC8-7B ........................................ 75 ........ 45 °C/W

NOTES:
5) Exceeding these ratings may damage the device.
6) The maximum allowable power dissipation is a function of the maximum junction temperature T_J(MAX), the junction-to-ambient thermal resistance θJA, and the ambient temperature T_A. The maximum allowable continuous power dissipation at any ambient temperature is calculated by P_D(MAX) = (T_J(MAX) - T_A)/θJA. Exceeding the maximum allowable power dissipation produces an excessive die temperature, causing the regulator to go into thermal shutdown. Internal thermal shutdown circuitry protects the device from permanent damage.
7) The device is not guaranteed to function outside of its operating conditions.
8) Measured on JESD51-7, 4-layer PCB.
ELECTRICAL CHARACTERISTICS
VCC = 15V, TJ = -40°C~125°C, min and max values are guaranteed by characterization, typical values are tested under 25°C, unless otherwise noted.

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Condition</th>
<th>Min</th>
<th>Typ</th>
<th>Max</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td>Supply Voltage Management (VCC)</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>VCC on threshold</td>
<td>VCC</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>VCC off threshold</td>
<td>VCC</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Operating current</td>
<td>IOP</td>
<td>fs = fs-min</td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>fs = 40kHz</td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Internal MOSFET (DRAIN)</td>
<td>Breakdown voltage</td>
<td>VBRDSS</td>
<td>700</td>
<td></td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>On state resistance</td>
<td>RDSon</td>
<td>VCC = 10V, IDS = 0.1A, TJ = 25°C</td>
<td>4.5</td>
<td>6.5</td>
<td></td>
<td>Ω</td>
</tr>
<tr>
<td>High-voltage current source supply current</td>
<td>IHV</td>
<td>VCC = 18V, VD = 80V, TJ = 25°C</td>
<td>1.8</td>
<td>2.2</td>
<td>2.6</td>
<td>mA</td>
</tr>
<tr>
<td>Leakage current</td>
<td>Ileak</td>
<td>VD = 400V, TJ = 25°C</td>
<td></td>
<td></td>
<td>11</td>
<td>μA</td>
</tr>
<tr>
<td>Internal MOSFET (SOURCE)</td>
<td>Maximum on time</td>
<td>tONmax</td>
<td>VSOURCE = 0V</td>
<td>25</td>
<td>40</td>
<td>55</td>
</tr>
<tr>
<td>Minimum switching frequency</td>
<td>fs-min</td>
<td></td>
<td></td>
<td>75</td>
<td>110</td>
<td></td>
</tr>
<tr>
<td>Current limit</td>
<td>VLimit-Max</td>
<td>fS ≥ fS-H</td>
<td>464</td>
<td>480</td>
<td>496</td>
<td>mV</td>
</tr>
<tr>
<td></td>
<td>VLimit-Min</td>
<td>fS ≤ fS-L</td>
<td>220</td>
<td>250</td>
<td>280</td>
<td>mV</td>
</tr>
<tr>
<td></td>
<td>fS to start the current foldback</td>
<td>fS-H</td>
<td>26</td>
<td>40</td>
<td>54</td>
<td>kHz</td>
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<tr>
<td></td>
<td>fS to end the current foldback</td>
<td>fS-L</td>
<td></td>
<td></td>
<td>20</td>
<td>kHz</td>
</tr>
<tr>
<td>Leading edge blanking</td>
<td>tLEB</td>
<td>190</td>
<td>300</td>
<td>410</td>
<td></td>
<td>ns</td>
</tr>
<tr>
<td>Feedback Input (FB)</td>
<td>FB input current</td>
<td>IFB</td>
<td>VFB = 4V, VCP = 2V</td>
<td>12</td>
<td></td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td>VFB = 4V, VCP = 1.5V</td>
<td>9</td>
<td></td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td>VFB = 4V, VCP = 0.8V</td>
<td>4.6</td>
<td></td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td>VFB = 4V, VCP = 0.2V</td>
<td>1.2</td>
<td></td>
<td></td>
</tr>
<tr>
<td>FB reference voltage</td>
<td>VFB</td>
<td></td>
<td>3.90</td>
<td>3.96</td>
<td>4.02</td>
<td></td>
</tr>
<tr>
<td>OLP threshold at sampled FB</td>
<td>VFBolp</td>
<td></td>
<td>1.4</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>OLP counter</td>
<td></td>
<td></td>
<td>768</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>FB sampling duration</td>
<td>tFB-SD</td>
<td></td>
<td>180</td>
<td>260</td>
<td>360</td>
<td></td>
</tr>
<tr>
<td>FB maximum sampling time</td>
<td>tFBS-Max</td>
<td>RSS = 0Ω, VLimit = 0.5V</td>
<td>2.60</td>
<td>3.62</td>
<td>4.9</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>RSS = 1kΩ, VLimit = 0.5V</td>
<td>1.85</td>
<td>2.72</td>
<td>3.65</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>RSS = 2kΩ, VLimit = 0.5V</td>
<td>3.8</td>
<td>5.5</td>
<td>7.2</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>RSS = 4kΩ, VLimit = 0.5V</td>
<td>5.3</td>
<td>7.2</td>
<td>9.3</td>
<td></td>
</tr>
<tr>
<td>FB minimum sampling time</td>
<td>tFBS-Min</td>
<td>RSS = 0Ω, VLimit = 0.25V</td>
<td>1.1</td>
<td>1.82</td>
<td>2.6</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>RSS = 1kΩ, VLimit = 0.25V</td>
<td>0.75</td>
<td>1.35</td>
<td>1.95</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>RSS = 2kΩ, VLimit = 0.25V</td>
<td>1.85</td>
<td>2.72</td>
<td>3.65</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>RSS = 4kΩ, VLimit = 0.25V</td>
<td>2.6</td>
<td>3.62</td>
<td>4.9</td>
<td></td>
</tr>
</tbody>
</table>
ELECTRICAL CHARACTERISTICS (continued)
VCC = 15V, TJ = -40°C~125°C, min and max values are guaranteed by characterization, typical values are tested under 25°C, unless otherwise noted.

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Condition</th>
<th>Min</th>
<th>Typ</th>
<th>Max</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td>ZCD threshold</td>
<td>VDCM</td>
<td></td>
<td>55</td>
<td>100</td>
<td>145</td>
<td>mV</td>
</tr>
<tr>
<td>FB open-circuit threshold</td>
<td>VFBope</td>
<td></td>
<td>-190</td>
<td>-110</td>
<td>-45</td>
<td>mV</td>
</tr>
<tr>
<td>OVP threshold at FB</td>
<td>VFBovp</td>
<td></td>
<td>5.7</td>
<td>5.96</td>
<td>6.3</td>
<td>V</td>
</tr>
<tr>
<td>FB OVP blanking time</td>
<td>tOVP-B</td>
<td></td>
<td>1</td>
<td>1.35</td>
<td>1.7</td>
<td>μs</td>
</tr>
</tbody>
</table>

Output Cable Compensation (CP)
Supply voltage on CP
VCP-Max
4
V

Thermal Shutdown
Thermal shutdown threshold (9)
140
°C
Thermal shutdown recovery hysteresis (9)
40
°C

NOTE:
9) The parameters are guaranteed by characterization.
<table>
<thead>
<tr>
<th>Pin #</th>
<th>Name</th>
<th>Description</th>
</tr>
</thead>
<tbody>
<tr>
<td>1</td>
<td>FB</td>
<td><strong>Feedback.</strong> The FB voltage determines the operation mode (CV mode or CC mode).</td>
</tr>
<tr>
<td>2</td>
<td>GND</td>
<td><strong>Ground.</strong></td>
</tr>
<tr>
<td>4</td>
<td>DRAIN</td>
<td><strong>Drain of the internal MOSFET.</strong> DRAIN is integrated with an internal high-voltage current source, which charges up VCC for start-up.</td>
</tr>
<tr>
<td>5</td>
<td>SOURCE</td>
<td><strong>Source of the internal MOSFET.</strong> Connect a current sense resistor to detect the MOSFET current for peak-current-mode control in CV and CC mode.</td>
</tr>
<tr>
<td>6</td>
<td>SS</td>
<td><strong>Select sampling time by different external resistor configurations.</strong></td>
</tr>
<tr>
<td>7</td>
<td>CP</td>
<td><strong>Output cable compensation.</strong> Connect a 1µF ceramic capacitor to CP as a low-pass filter. The compensation voltage can be adjusted by the resistor divider. CP can also be used to select the secondary duty limitation by different external resistor configurations.</td>
</tr>
<tr>
<td>8</td>
<td>VCC</td>
<td><strong>Supply voltage.</strong> When VCC is lower than a certain level, the internal high voltage current source is turned on to charge up VCC. When VCC is charged to a certain level by the internal high-voltage current source, the IC begins working. In addition to the bulk capacitor, a 0.1µF ceramic capacitor can be connected as close to VCC as possible to decouple the noise disturbance.</td>
</tr>
</tbody>
</table>
TYPICAL CHARACTERISTICS

VCC On Threshold vs. Temperature

VCC Off Threshold vs. Temperature

High-Voltage Current Source Supply Current @ V_D = 80V vs. Temperature

Leakage Current @ V_D = 400V vs. Temperature

Breakdown Voltage vs. Temperature

Operating Current @ F_s, min vs. Temperature
TYPICAL CHARACTERISTICS (continued)

On-State Resistance vs. Temperature

Operating Current @ \( f_s = 40kHz \) vs. Temperature

FB Reference Voltage vs. Temperature

Current Limit vs. Temperature

ZCD Threshold vs. Temperature

FB Open-Circuit Threshold vs. Temperature
TYPICAL CHARACTERISTICS (continued)

Minimum Switching Frequency vs. Temperature

FB Maximum Sampling Time @ $R_{ss} = 0\Omega$
vs. Temperature

FB Minimum Sampling Time @ $R_{ss} = 0\Omega$
vs. Temperature
TYPICAL PERFORMANCE CHARACTERISTICS

Performance waveforms are tested on the evaluation board in the Design Example section. $V_{IN} = 230V_{AC}$, $V_{OUT} = 5V$, $I_{OUT} = 2A$, unless otherwise noted.

No-Load Consumption

![No-Load Consumption Graph](image)

Efficiency

![Efficiency Graph](image)

Conducted EMI

$V_{IN} = 115V_{AC}$, L Line

![Conducted EMI L Line Graph](image)

Conducted EMI

$V_{IN} = 230V_{AC}$, L Line

![Conducted EMI L Line Graph](image)

Conducted EMI

$V_{IN} = 115V_{AC}$, N Line

![Conducted EMI N Line Graph](image)

Conducted EMI

$V_{IN} = 230V_{AC}$, N Line

![Conducted EMI N Line Graph](image)
TYPICAL PERFORMANCE CHARACTERISTICS (continued)
Performance waveforms are tested on the evaluation board in the Design Example section. 
\( V_{IN} = 230V_{AC} \), \( V_{OUT} = 5V \), \( I_{OUT}=2A \), unless otherwise noted.

Steady State 
\( V_{IN} = 265V_{AC} \)

Power On 
\( V_{IN} = 265V_{AC} \)

OLP Entry

OLP Recovery

OLP Power On

Short-Circuit Entry
TYPICAL PERFORMANCE CHARACTERISTICS (continued)  
Performance waveforms are tested on the evaluation board in the Design Example section. $V_{IN} = 230V_{AC}$, $V_{OUT} = 5V$, $I_{OUT} = 2A$, unless otherwise noted.

**Short-Circuit Recovery**

CH1: $V_{DS PRI}$  
200V/div.  

CH2: $V_{CC}$  
10V/div.  

CH3: $V_{OUT}$  
5V/div.  

400ms/div.

**Short-Circuit Power On**

CH1: $V_{DS PRI}$  
200V/div.  

CH2: $V_{CC}$  
10V/div.  

CH3: $V_{OUT}$  
5V/div.  

400ms/div.
Figure 1: Functional Block Diagram
OPERATION

The MP024-10 is a primary-side flyback regulator that provides accurate constant voltage and constant current regulation without an optocoupler or secondary feedback circuit. The regulator is designed to operate with a minimal number of external components.

Start-Up

Initially, the IC is self-supplied by the internal high-voltage current source, which is drawn from DRAIN. The internal high-voltage current source turns off for better efficiency once VCC reaches the VCC on threshold (V_CCH). Afterward, the power supply is taken over by the auxiliary winding of the transformer. When VCC falls below the VCC off threshold (V_CC_L), the IC stops switching, and the internal high-voltage current source turns on again (see Figure 2).

Peak-Current Control on the Primary Side

A current sense resistor (R_S) is used to sense the primary current I_p(t) (see Figure 3). The current rises linearly at a rate shown in Equation (1):

\[
\frac{dI_p(t)}{dt} = \frac{V_m}{L_m}
\]  

(1)

When the current I_p(t) rises up to I_pk, the MOSFET turns off. Calculate I_pk with Equation (2):

\[
I_{pk} = \frac{V_{IPK}}{R_S}
\]  

(2)

The energy stored in the inductor (L_m) within each cycle can be calculated with Equation (3):

\[
E = \frac{1}{2} L_m \times I_{pk}^2
\]  

(3)

The power transferred from the input to the output can be calculated with Equation (4):

\[
P = \frac{1}{2} L_m \times I_{pk}^2 \times f_s
\]  

(4)

Where f_s is the switching frequency.

In constant current operation, the reference for I_pk is fixed at V_Limit-Max. In constant voltage operation, I_pk is modulated by the switching frequency (see Figure 4).
Constant Voltage (CV) Operation

In constant voltage (CV) mode, the MP024-10 detects the output voltage from FB and generates the switching frequency to regulate the output voltage.

To regulate the output voltage on the primary side, FB uses a resistor divider to sample the auxiliary winding voltage \( V_{\text{aux}} \). The relationship between \( V_{\text{aux}} \) and the output voltage \( V_o \) can be calculated with Equation (5):

\[
V_{\text{aux}} = \frac{N_{\text{aux}}}{N_s} \times (V_o + V_D)
\]  

(5)

Where \( V_D \) is the forward drop voltage of the secondary diode.

During the conduction time of the secondary diode, the difference between the output voltage and the voltage on the secondary winding is not constant, since \( V_D \) varies with the current flowing through the diode. To compensate for the voltage drop difference, the sampling time decreases gradually from \( t_{\text{FBS-Max}} \) to \( t_{\text{FBS-Min}} \) as the current limitation folds back from \( V_{\text{Limit-Max}} \) to \( V_{\text{Limit-Min}} \) (see Figure 5).

![Figure 5: Auxiliary Winding Voltage](image)

The FB sampling time is able to be customized with different resistor values connected to SS (see Figure 6). See the Electrical Characteristics table on page 5 for all available choices for the sampling time. The entire customization process is completed before start-up and stored in a register, so it does not have any influence on the normal operation.

![Figure 6: External Resistor for Sampling Time Customization](image)

The sampling should be chosen almost at the end of the secondary diode conduction period for accurate CV regulation.

Constant Current (CC) Operation

Figure 7 shows the secondary current waveforms.

![Figure 7: Secondary Current Waveform](image)

In constant current (CC) operation, \( I_{\text{pk}} \) is fixed, and the CC loop control function maintains a fixed ratio between the secondary diode on time \( t_{\text{ons}} \) and the switching cycle. The fixed ratio limits the maximum duty of the secondary side diode on time as shown in Equation (6):

\[
\frac{t_{\text{ons}}}{T} = D_{S-\text{Max}}
\]  

(6)

The relationship between the output constant-current and the secondary peak current \( I_{\text{pks}} \) is shown in Equation (7):

\[
I_{\text{out}} = \frac{1}{2} I_{\text{pks}} \frac{t_{\text{ons}}}{t_{\text{ons}} + t_{\text{offs}}} = \frac{1}{2} I_{\text{pks}} D_{S-\text{Max}}
\]  

(7)

When the secondary diode is turned on, the peak current on the secondary side can be calculated with Equation (8):

\[
I_{\text{pks}} = \frac{N_p}{N_s} I_{\text{pK}}
\]  

(8)

The output current regulation is shown in Equation (9):

\[
I_{\text{out}} = \frac{1}{2} \frac{N_s}{N_p} I_{\text{pk}} D_{S-\text{Max}}
\]  

(9)

For different applications with different kinds of output voltages, \( D_{S-\text{Max}} \) can be customized from CP. If CP is connected with a capacitor directly or shorted to GND, \( D_{S-\text{Max}} \) remains at a default value of 0.4.
If CP is connected with a resistor, then there are several options for the CP and $D_{S\text{ Max}}$ combination (see Figure 8).

![Figure 8: External Configuration of CP](image)

Table 1 shows all available choices for $D_{S\text{ Max}}$. The entire customization process is completed before start-up and latched in a register, so it does not have any influence on the normal operation.

<table>
<thead>
<tr>
<th>$R_{CP}/C_{CP}$</th>
<th>$D_{S\text{ Max}}$</th>
</tr>
</thead>
<tbody>
<tr>
<td>0Ω/NC</td>
<td>0.4</td>
</tr>
<tr>
<td>10kΩ/NC</td>
<td>0.3</td>
</tr>
<tr>
<td>20kΩ/NC</td>
<td>0.35</td>
</tr>
<tr>
<td>40kΩ/NC</td>
<td>0.5</td>
</tr>
<tr>
<td>NC/1μF</td>
<td>0.4</td>
</tr>
</tbody>
</table>

To enable the overload protection (OLP) function in CC mode, the sampling on the FB voltage should be running, and the sampling time should be fixed at $t_{FB\text{ Max}}$.

**Leading-Edge blanking**
The MP024-10 uses a leading-edge blanking period when the MOSFET turns on. Leading-edge blanking is used to prevent a false termination of the switching pulse caused by the turn-on current spike. During this blanking period, the current sense comparator is disabled, and the MOSFET cannot be turned off.

**Discontinuous Conduction Mode (DCM) Detection**
The MP024-10 is designed to operate in discontinuous conduction mode (DCM) in both CV and CC modes. To avoid operating in continuous conduction mode (CCM), the MP024-10 implements a zero-current detection function internally with a threshold of $V_{DCM}$. The IC does not begin the next cycle until ZCD is detected.

During normal operation, the blanking time for ZCD is synchronized with the FB sampling time (i.e.: ZCD always starts after the sampling phase is done). There is also a soft-start (SS) function on the ZCD blanking time that prevents ZCD from being falsely triggered when the output capacitor is not charged up. During the start-up period, the blanking time for ZCD gradually shrinks from $t_{S\text{ STP}}$ (10μs) to the FB sampling time in three cycles.

**Protection Features (OVP, OCKP, SSP, and OLP)**
The MP024-10 includes over-voltage protection (OVP), open-circuit protection (OCKP), sensing-short protection (SSP), and overload protection (OLP). If the voltage at FB exceeds $V_{FB\text{ OVP}}$, OVP is triggered. If $V_{FB\text{ OVP}}$ cannot be monitored for each cycle, OCKP is triggered. If the maximum turn on time is reached, SSP is triggered. If the sampled FB voltage is lower than $V_{FB\text{ OVP}}$ for 128 consecutive cycles, OLP is triggered. The MP024-10 immediately shuts down the driving signals and enters hiccup mode when any of these protection features are triggered and resumes normal operation when the fault has been removed.

OLP is not enabled until the soft-start period of the ZCD blanking time is finished.

**Over-Temperature Protection (OTP)**
When the junction temperature of the IC exceeds the thermal shutdown threshold, over-temperature protection (OTP) is triggered, and the IC stops switching. The MP024-10 resumes normal operation when the junction temperature drop exceeds the thermal shutdown hysteresis.

**Output Cable Compensation**
The MP024-10 has an internal output cable compensation circuit (see Figure 9). A switching signal ($V_{\text{Limit}*\text{ON}}$) is generated internally and is synchronized with the switching frequency. The duty on time of this signal is $t_{\text{ON}}$, and the amplitude of this signal is proportional to the current limit threshold. The switching signal is output to CP through a 1MΩ resistor. A low-pass filter can be implemented by placing an external capacitor on CP, and a DC voltage ($V_{CP}$) that is proportional to the output current can be derived on CP.

An internal current sinking into FB is proportional to $V_{CP}$, so the voltage drop on the upper resistor of the divider implements the output cable compensation function.
Determine the compensation voltage with Equation (10):

\[ V_{FCP} = \frac{8 \times V_{Limit} \times D_s \times 2 \times R_{UP} \times N_s}{N_{P_AU}} \times 300 \times 10^3 \] (10)

Where \( V_{FCP} \) is the secondary-side compensation voltage drop, \( D_s \) is the secondary-diode duty cycle, \( R_{UP} \) is the upper resistor of the resistor divider, \( N_s \) is the number of turns for the secondary-side transformer windings, \( N_{P_AU} \) is the number of transformer auxiliary winding turns, and \( V_{Limit} \) is the current limit.

For example, to calculate the maximum output cable compensation in CC condition, use \( D_s = D_{S-Max} \) (when CP function is used, \( D_{S-Max} \) is 0.4) and \( V_{Limit} = V_{Limit-Max} \) (typically 480mV) in the formula. The compensation voltage drops as \( V_{Limit} \) or \( D_s \) decrease along with the load current. The CP voltage is \( 8 \times V_{Limit} \times D_s \).

Connect a 1μF capacitor to CP for cable compensation. Since CP is also used for \( D_{S-Max} \) customization, the cable compensation function is only available when CP is connected to the capacitors directly. If there is any non-zero resistor connected to CP, all of the internal blocks related to the cable compensation function are disabled and there is no current sinking into FB.
APPLICATION INFORMATION

Input Filter
The input filter helps to maintain the bus voltage when the AC input voltage is low.

Figure 10 shows the typical input filter of an application with a low power range. The bulk capacitors (C1 and C2) filter the rectified AC input. Usually, C1 and C2 are set at 2µF/W to 3µF/W for a universal input condition. For 230VAC single-range applications, cut the capacitor values in half. The inductor (L) forms a pi (π) filter with C1 and C2 to restrain the differential mode EMI noise. The resistor (R) in parallel with L dampens the mid-frequency band EMI noise, if necessary. Normally, R is 1kΩ to 10kΩ.

Figure 11 shows the typical DC bus voltage waveform after the rectifier.

![Figure 10: Input Filter](image)

![Figure 11: DC Input Voltage Waveform](image)

Output Capacitor
Low or very low ESR output capacitors are recommended to meet the output voltage ripple requirements. Low ESR capacitors improve the output voltage regulation accuracy at high or low temperatures and can provide better efficiency than high ESR output capacitors.

Output Diode Or Synchronous Rectifier
Schottky diodes are recommended for their fast switching speed and low forward voltage drop for better high or low temperature CV regulation and efficiency.

If lower average efficiency (3% to 4%) is acceptable, replace the output diode with a fast or ultra-fast diode to reduce cost. Re-adjust the resistor divider values for an accurate output voltage since the forward voltage drop is higher than the Schottky diode.

If the circuit has a high efficiency requirement, it is recommended to use a synchronous rectifier (SR) instead. The MP6906 is a suitable SR controller where the output voltage is low and there is no need for a secondary auxiliary winding (see Figure 12). The MP6906 is available in a SOT23-6 package, which only requires few extra PCB dimensions and external components.

Leakage Inductance
The transformer’s leakage inductance decreases system efficiency and affects either the output current or voltage constant precision. The transformer structure can be optimized to minimize the leakage inductance. The leakage inductance should be less than 5% of the primary inductance.
RCD Snubber
The transformer’s leakage inductance causes MOSFET drain voltage spikes and excessive ringing on the drain voltage waveform, which affects the output voltage sampling after the primary MOSFET turns off.

The RCD snubber circuit limits the drain voltage spike (see Figure 13).

![Figure 13: RCD Snubber](image)

Select an appropriate $R_{SN}$ and $C_{SN}$ value to meet voltage spike requirements and improve system operation.

The power dissipated in the snubber circuit can be approximated with Equation (12):

$$P_{SN} = \frac{1}{2} L_K I_{PK}^2 \frac{V_{SN}}{V_{SN} - N_{PS} V_O} f_s$$  \hspace{1cm} (12)

Where $L_K$ is the leakage inductance, $V_{SN}$ is the clamp voltage, and $N_{PS}$ is the turn ratio of the primary-to-secondary side.

Since $R_{SN}$ consumes the majority of the power, calculate $R_{SN}$ with Equation (13):

$$R_{SN} = \frac{V_{SN}^2}{P_{SN}}$$  \hspace{1cm} (13)

The maximum ripple of the snubber capacitor voltage is then calculated with Equation (14):

$$\Delta V_{SN} = \frac{V_{SN}}{C_{SN} R_{SN} f_s}$$  \hspace{1cm} (14)

Generally, a 15% ripple is reasonable.

Select a time constant ($t = R_{SN} \cdot C_{SN}$) below 0.1ms for better CV sampling. Calculate $C_{SN}$ using Equation (14).

The RCD resistor is a trade-off between the power loss and the acceptable clamp voltage in practical applications.

The damping resistor in series with the RCD has a relatively large value to prevent any excessive voltage ringing that can affect the CV sampling and increase the output ripple. Use a damping resistor value in the range of 100Ω to 500Ω to restrain the drain voltage ringing.

Resistor Divider
For better application performance, select the resistor divider’s total value with in the range of 10kΩ to 100kΩ. Smaller resistors will draw larger current from the auxiliary winding, which increases the no-load consumption, and larger resistors may pick up noise from adjacent components.

If there is oscillation or noise disturbing the FB sampling, an R-C filter can be inserted between the resistor divider and FB to achieve a stable voltage. The $C_{FB}$ value is recommended to be several pF, and $R_{FB}$ is recommended to be between 1kΩ and 2kΩ. $R_{FB}$ can also limit substrate injection current effects (see Figure 14).

![Figure 14: Feedback Resistor Divider Circuit](image)

For accurate CV regulation, the accuracy of these feedback resistors should be at least 1%.

Dummy Load
When the system operates without any load, the output voltage rises above the normal operation because of the minimum switching frequency limitation. Use a dummy load for good load regulation. The dummy load is a trade-off between efficiency and load regulation. For example, a large dummy load can deteriorate efficiency and no-load consumption. For most applications, a dummy load of several mW is reasonable.
Maximum Switching Frequency

The maximum switching frequency should be limited by the sampling point. The relationship between $R_{SS}$ and the sampling time point is shown in the Electrical Characteristics table on page 5. The secondary on time must be longer than the maximum $T_{FBS\text{-}Max}$. Calculate $T_{S\text{-}ON}$ with Equation (15):

$$T_{S\text{-}ON} = \frac{N_s \cdot L_w}{N_p \cdot (V_o + V_d)} > t_{FBS\text{-}Max} + t_{FB\text{-}SD} \quad (15)$$

Where $T_{FBS\text{-}Max}$ is the FB maximum sampling time, and $t_{FB\text{-}SD}$ is the FB sampling duration.

Combine Equation (14) and the relationship of $R_{CP}$ and $D_{S\text{-}Max}$ shown in Table 1 to fix the maximum switching frequency.

PCB Layout Guidelines

Efficient PCB layout is critical for stable operation, good EMI, and good thermal performance. For best results, refer to Figure 15 and follow the guidelines below.

1. Minimize the loop area formed by the input capacitor, the transformer’s primary winding, the MOSFET drain and source of the MP024-10, and the sensing resistor to reduce EMI noise.
2. Minimize the voltage jumping area, such as the MOSFET drain, the anode of the secondary diode, etc. for better EMI.
3. Minimize the clamp circuit loop to reduce EMI.
4. Minimize the secondary loop area of the output diode and output filter to reduce EMI noise.
5. Provide sufficient copper areas at the cathode terminal of the output diode to act as a heat sink.
6. Place the AC input away from the switching nodes to minimize any noise coupling that may bypass the input filter.
7. Place the bypass capacitor as close to the IC as possible.
8. Place the feedback resistors next to FB and minimize the feedback sampling loop to minimize noise coupling.
9. Use a single-point connection at the negative terminal of the input filter capacitor for the IC GND and bias winding return.

Table 2: Design Example

<table>
<thead>
<tr>
<th>$V_{IN}$</th>
<th>85Vac~265Vac, 47Hz/63Hz</th>
</tr>
</thead>
<tbody>
<tr>
<td>$V_{OUT}$</td>
<td>5V</td>
</tr>
<tr>
<td>$I_{OUT}$</td>
<td>2A</td>
</tr>
</tbody>
</table>

Figure 16 shows the detailed application schematic. For more device applications, please refer to the related evaluation board datasheets.
TYPICAL APPLICATION CIRCUIT

Figure 16: Universal Input, 5V/2A Output
Figure 17: Flow Chart
SIGNAL TIMING SEQUENCE WAVEFORM

Figure 18: Start-Up Sequence

Figure 19: Protection Sequence
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PACKAGE INFORMATION

SOIC8-7B

TOP VIEW

FRONT VIEW

SIDE VIEW

NOTE:

1) CONTROL DIMENSION IS IN INCHES. DIMENSION IN BRACKET IS IN MILLIMETERS.
2) PACKAGE LENGTH DOES NOT INCLUDE MOLD FLASH, PROTRUSIONS, OR GATE BURRS.
3) PACKAGE WIDTH DOES NOT INCLUDE INTERLEAD FLASH OR PROTRUSIONS.
4) LEAD COPLANARITY (BOTTOM OF LEADS AFTER FORMING) SHALL BE 0.004" INCHES MAX.
5) JEDEC REFERENCE IS MS-012.
6) DRAWING IS NOT TO SCALE.